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Published in:
I E E E Transactions on Power Electronics

DOI (link to publication from Publisher):
[10.1109/TPEL.2018.2848668](https://doi.org/10.1109/TPEL.2018.2848668)

Publication date:
2019

Document Version
Accepted author manuscript, peer reviewed version

[Link to publication from Aalborg University](#)

Citation for published version (APA):
Wang, H., & Wang, H. (2019). A Two-terminal Active Inductor with Minimum Apparent Power for the Auxiliary Circuit. *I E E E Transactions on Power Electronics*, 34(2), 1013-1016. Article 8387810.
<https://doi.org/10.1109/TPEL.2018.2848668>

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Letters

A Two-terminal Active Inductor with Minimum Apparent Power for the Auxiliary Circuit

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Abstract—This letter proposes a concept of a two-terminal active inductor with minimum apparent power processed by the auxiliary circuits, which are implemented by power semiconductor switches and passive elements. It has the same level of convenience as a passive inductor with two power terminals only. Compared with a conventional inductor with the same equivalent inductance and current rating, the energy storage requirement of the inductor can be reduced significantly, as well as the weight and volume. The auxiliary circuit in the active inductor processes both partial voltage and partial current, with the lowest apparent power rating compared to existing solutions. A case study for the DC-link filter inductor in a three-phase diode-bridge rectifier is discussed. Proof-of-concept experimental results are given to verify the functionality and effectiveness of the proposed active inductor.

Index Terms—Active circuits, inductor, impedance element, power converter

I. INTRODUCTION

POWER semiconductor, capacitor and inductor are the basic elements in power electronic systems. Passive elements such as inductor and capacitor still have considerably lower power density compared to active switches [1]. Based on the duality of a two-terminal active capacitor concept proposed in [2], this letter proposes a two-terminal active inductor. It could achieve the same equivalent impedance characteristics of interest as a passive inductor while with a reduced inductive energy storage, implying the potential to size and weight reduction. Fig. 1 shows the duality between the two concepts. The proposed active inductor concept distinguishes itself from the ones discussed in [1] and [3–5] from two aspects: 1) it has two terminals only same as a conventional passive inductor without any external feedback signal and power supply, and 2) the auxiliary circuit in the proposed inductor processes the lowest apparent power, which is the theoretical minimum limit. The proposed active inductor can be controlled to have its impedance characteristics equivalent to a bulky passive inductor within a certain frequency range of interest.

Figs. 2 (a) and (b) show the concept of the existing active inductors and the proposed one, respectively. Terminals A and B are the ones that a passive inductor would be connected to a power electronic circuit. The current i_{AB} is an AC current or with DC bias, consisting of the main frequency component

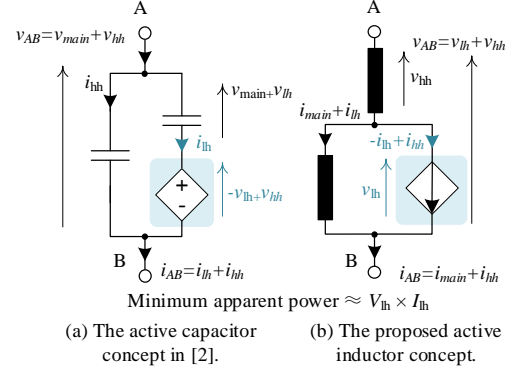


Fig. 1. The duality between the two-terminal active capacitor in [2] and the proposed active inductor concept. v_{AB} , i_{AB} are the instantaneous terminals' voltage and current, respectively. v_{main} , v_{lh} and v_{hh} are the instantaneous main voltage, low-frequency and high-frequency harmonic voltage, respectively. i_{main} , i_{lh} , and i_{hh} are the instantaneous main current, low-frequency and high-frequency harmonic current, respectively. V_{lh} and I_{lh} are the Root Mean Square (RMS) values of v_{lh} and i_{lh} , respectively.

i_{main} and undesirable ripples, depending on specific applications. The auxiliary circuit (i.e., the controlled-voltage source) in Fig. 2 (a) generates a voltage that follows the undesirable voltage ripples of v_{AB} , usually the low-frequency harmonics of interest (i.e., v_{lh}). Therefore, the inductor L_f has high-frequency harmonics only if the auxiliary circuit operates ideally. It can be noted that the auxiliary circuit needs to process the entire current i_{AB} , approximated as i_{main} if the high-frequency harmonics i_{hh} is ignored. Different from the concept shown in Fig. 2 (a), the proposed auxiliary circuit generates a controlled-current source as shown in Fig. 2 (b) and processes a partial current only. Moreover, none of the methods presented in [1] and [3–5] can implement a plug-and-play active inductor since they have more terminals, such as external feedback signals and auxiliary power supplies for the controller and gate drivers. This letter presents the concept of the proposed active inductor and one of the implementations by applying the self-power method presented in [2] and a current control strategy without external feedback signal.

II. THE CONCEPT AND AN IMPLEMENTATION OF THE TWO-TERMINAL ACTIVE INDUCTOR

A. Concept of the Two-terminal Active Inductor

As shown in Fig. 2 (b), the proposed active inductor consists of a high-frequency inductor L_f , a low-frequency inductor L_l ,

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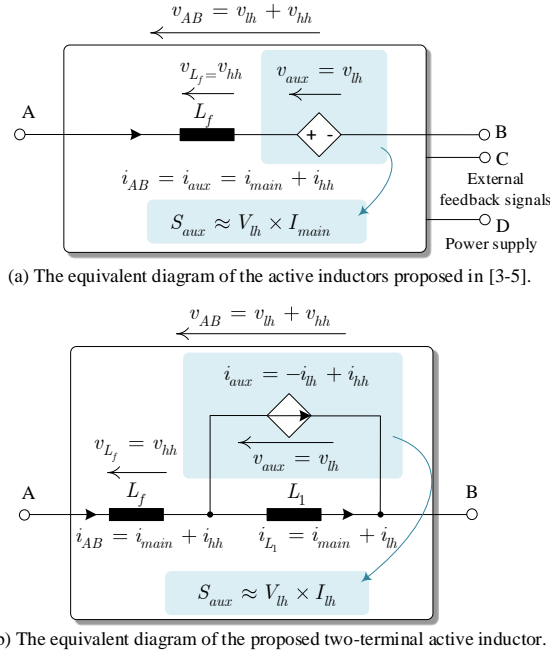


Fig. 2. The equivalent diagrams of (a) existing active inductors and (b) the proposed two-terminal active inductor. v_{AB} , i_{AB} , v_{aux} and i_{aux} are the instantaneous voltage and current of the terminals and the auxiliary circuit, respectively. v_{lh} and v_{hh} are the instantaneous low-frequency and high-frequency harmonic voltage, respectively. i_{main} , i_{lh} , and i_{hh} are the instantaneous main current, low-frequency harmonic current and high-frequency harmonic current, respectively. V_{lh} , I_{lh} and I_{main} are RMS values of low-frequency voltage, low-frequency current and main current, respectively. S_{aux} is the apparent power of the auxiliary circuit.

and a controlled-current source connected in parallel with L_1 . The controlled-current source i_{aux} is equal to the undesirable low-frequency current harmonics i_{lh} of L_1 with out of phase and high-frequency harmonics i_{hh} . The voltage across the controlled-current source is equal to the undesirable low-frequency voltage harmonics of v_{aux} . Therefore, the auxiliary circuit used to implement the controlled-current source processes the partial voltage of v_{AB} and the partial current of i_{AB} only, as indicated in Fig. 2 (b).

A current control strategy is proposed for the auxiliary circuit which will be discussed specifically in Part B of Section II. It is based on internal voltage and current information of the auxiliary circuit. A self-power method implemented in [2] is applied for this study, which obtains the power for the digital controller and gate drivers from the active power switches in the auxiliary circuit. Therefore, the proposed concepts eliminate the use of external feedback signal and auxiliary power supply. The active inductor has two power terminals A and B only, making it as convenient as a conventional inductor.

B. An Implementation of the Two-terminal Active Inductor Concept

One of the possible implementations of the proposed active inductor concept is shown in Fig. 3. A full-bridge bi-directional converter is used as the auxiliary circuit. C_1 is the DC-link capacitor of the auxiliary circuit and L_2 is the smoothing inductor. A self-power unit is used to obtain the power for gate drivers and controller in the active circuit

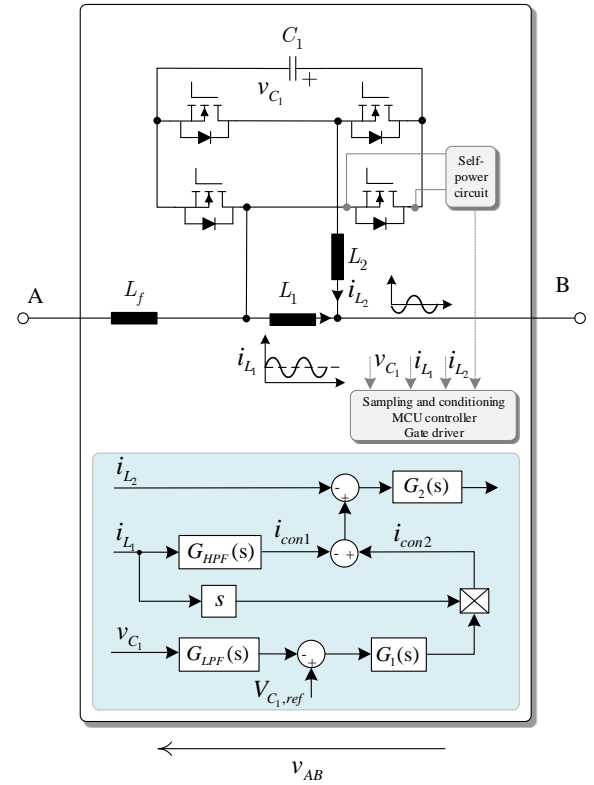


Fig. 3. An implementation of the proposed two-terminal active inductor with a current control strategy.

from the drain-source terminals of a MOSFET, which can be referred to [2]. The objective is to control i_{L2} to be out of phase with the harmonic component in i_{L1} and with the same amplitude. The reference of i_{L2} contains two parts: 1) i_{con1} is the extracted harmonic component of i_{L1} which is used to modulate the converter to generate the desired i_{L2} ; 2) i_{con2} is used to stabilize v_{C1} . The phase of i_{con2} and i_{con1} is synchronized (i.e., 90° phase shift with i_{con1}), in order to absorb active power from external circuits through terminals A and B to compensate the power loss of the auxiliary circuit. Based on small-signal analysis [6], the impedance of the active inductor is obtained as

$$Z_{AB} = \frac{\Delta v_{AB}(s)}{\Delta i_{AB}(s)} = \frac{\Delta i_{L1}(s)L_1s}{\Delta i_{L1}(s) + \Delta i_{L1}(s)G_r(s)} = \frac{L_1s}{1 + G_r(s)} \quad (1)$$

where $\Delta v_{AB}(s)$, $\Delta i_{AB}(s)$, $\Delta i_{L1}(s)$ and $\Delta i_{L2}(s)$ are the AC perturbations. $G_r(s)$ is the transfer function from $\Delta i_{L1}(s)$ to $\Delta i_{L2}(s)$ as presented by (2). M is the modulation index. I_{L2} and V_{C1} are the Root Mean Square (RMS) values of the inductor current i_{L2} and capacitor voltage v_{C1} , respectively. $G_{HPF}(s)$ and $G_{LPF}(s)$ are the high pass filter (HPF) and low pass filter (LPF) in the conditioning circuits of i_{L1} and v_{C1} , respectively. $G_1(s)$ and $G_2(s)$ are the PID controllers of the power loss compensation loop and current control loop, respectively.

III. APPLICATION OF THE ACTIVE INDUCTOR IN A THREE-PHASE DIODE-BRIDGE RECTIFIER

A. Component Sizing

The specification of the case study is shown in Table I.

$$G_r(s) = \frac{\Delta i_{L_2}(s)}{\Delta i_{L_1}(s)} = \frac{C_1 L_1 s^2 + G_1(s) G_{L_{PF}}(s) G_2(s) L_1 I_{L_2} s - C_1 G_{HPF}(s) G_2(s) V_{C_1} s + M G_{HPF}(s) G_2(s) I_{L_2}}{C_1 L_2 s^2 + G_1(s) G_{L_{PF}}(s) G_2(s) L_2 I_{L_2} s + C_1 G_2(s) V_{C_1} s + M^2 + M G_1(s) G_{L_{PF}}(s) G_2(s) V_{C_1} - M G_2(s) I_{L_2}} \quad (2)$$

TABLE I
SPECIFICATION OF A 900 W THREE-PHASE DIODE-BRIDGE RECTIFIER WITH A TWO-TERMINAL ACTIVE INDUCTOR.

Parameters	Description
Three-phase diode-bridge rectifier	
P	Power rating, 900 W
v_{AC}	AC voltage (RMS), 110 V
f_a	Fundamental frequency, 50 Hz
I_{main}	Main component current, 3.8 A
$V_{DC-link}$	DC-link voltage, 240 V
Two-terminal active inductor	
C_1	470 μF / 35 V
L_1	NCC EKY-350ELL471MJ20S
L_2	DC inductor L_1 , 8 mH/ 6 A
L_f	AC inductor L_2 , 100 μH / 2 A
α	Current ripple ratio of DC-link current, 17 %
β	Current ripple ratio of L_1 , 60 %

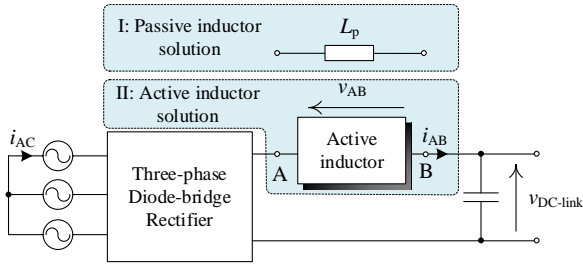


Fig. 4. System diagram of the three-phase diode-bridge rectifier with passive or active inductor solution.

The diagram of the three-phase diode-bridge rectifier with a two-terminal active inductor is shown in Fig. 4. The high-frequency current harmonics and high-frequency filter L_f are not considered in the following discussions. The inductance of L_1 is

$$L_1 = \frac{2\sqrt{2}V_{lh}}{\omega_{lh}\beta I_{main}} \quad (3)$$

where V_{lh} is the RMS value of low-frequency voltage harmonic of interest. ω_{lh} is the angular frequency of the low-frequency harmonic. β is the ripple current ratio of L_1 . $\beta = \frac{I_{L_1-pp}}{I_{main}}$, where I_{L_1-pp} is the peak-to-peak value of the ripple current of L_1 . Therefore, the value of β determines the processed current in the auxiliary circuit. There is a trade-off between its apparent power and the inductance value L_1 . In practice, there are high-frequency current harmonics in i_{aux} due to the non-ideal operation of the auxiliary circuit. The high-frequency current level depends on the values of C_1 , L_2 , and the switching frequency of the auxiliary circuit, which is not discussed here for the sake of simplicity. With the conventional inductor solution, the required inductance L_p is

$$L_p = \frac{2\sqrt{2}V_{lh}}{\omega_{lh}\alpha I_{main}} \quad (4)$$

where α is the ripple current ratio limit of i_{AB} (i.e., the DC-link current in the case study). The apparent power ratio between the auxiliary circuit of the proposed active inductor

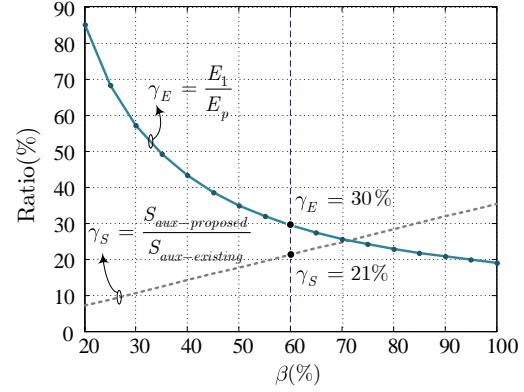


Fig. 5. Relation between ripple current ratio β of L_1 , apparent power ratio γ_S and energy storage ratio γ_E with 17 % current ripple ratio α .

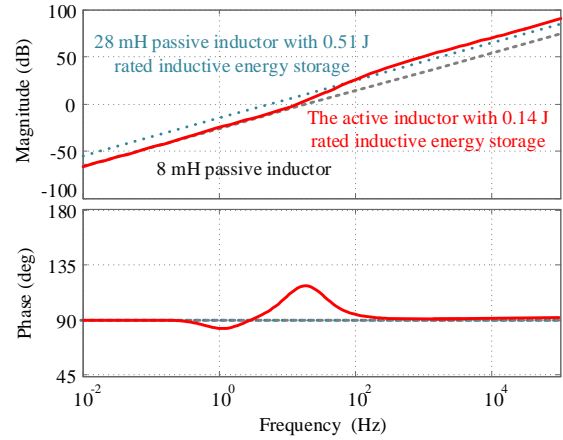


Fig. 6. Impedance curves of an active inductor with 0.14 J rated inductive energy storage and a passive inductor with 0.51 J rated energy storage.

in Fig. 2 (b) and the one of existing solutions in Fig. 2 (a) is

$$\gamma_S = \frac{S_{aux-proposed}}{S_{aux-existing}} = \frac{V_{lh} \times \frac{\beta}{2\sqrt{2}} I_{main}}{V_{lh} \times I_{main}} = \frac{1}{2\sqrt{2}} \beta. \quad (5)$$

The actual energy storage ratio between L_1 of the active inductor and L_p of the passive solution is

$$\gamma_E = \frac{E_1}{E_p} = \frac{\frac{1}{2} L_1 \left(\sqrt{I_{main}^2 + \left(\frac{\beta}{2\sqrt{2}} I_{main} \right)^2} \right)^2}{\frac{1}{2} L_p \left(\sqrt{I_{main}^2 + \left(\frac{\alpha}{2\sqrt{2}} I_{main} \right)^2} \right)^2} = \frac{\alpha(8 + \beta^2)}{\beta(8 + \alpha^2)}. \quad (6)$$

In Fig. 5, $\alpha = 17\%$ is selected as a case to investigate the relation between β , γ_S and γ_E . With $\beta = 60\%$, $L_p = 27.9$ mH, $L_1 = 7.9$ mH, $\gamma_E = 30\%$, and $\gamma_S = 21\%$. Considering the design margin, the passive components used in experimental setup are $L_p = 28$ mH/ 6 A with 0.51 J rated energy storage, $L_1 = 8$ mH/ 6 A with 0.14 J rated energy storage. Fig. 6 shows the impedance curve of the active inductor based on

the following parameters: $M = 0.9$, $I_{L2} = 0.9$ A, $V_{C1} = 25$ V, $\omega_{lh} = 1884$ rad/sec, $G_{HPF}(s) = 0.02s/(0.02s + 1)$ and $G_{LPF}(s) = 1/(0.1s + 1)$, $G_1(s) = (0.1s + 2)/s$ and $G_2(s) = (0.005s^2 + 0.8s + 10)/s$. In the frequency range below 50 Hz, the impedance characteristics of the active inductor is equivalent to a 8 mH inductor, which is determined by L_1 . For a frequency at 100 Hz or above, the impedance of the active inductor is slightly higher than a 28 mH passive inductor. It implies that the active inductor can achieve a comparable equivalent inductance with 27.5 % rated inductive energy storage in the presented case study.

B. Experimental Results

Fig. 7 shows the experimental waveforms of the diode-bridge rectifier with the implemented two-terminal active inductor with 0.14 J rated inductive energy storage. The power loss of the active inductor is 4 W in the presented case study, which is 0.44 % with respect to the apparent power of the main system. Fig. 7 (a) shows a 18 % current ripple of the DC link, with the peak-to-peak value of 0.7 A, which is slightly higher than the theoretical analysis due to the existence of high-frequency ripple current harmonics. Fig. 7 (b) shows the comparative results of the rectifier with a passive inductor with 0.51 J rated energy storage. The difference in the DC-link current ripple is negligible. The apparent power handled by the auxiliary circuit is 21 % of that in existing solutions shown in Fig. 2 (a). Fig. 8 presents the key waveforms of the active inductor. It can be noted that the ripple current of i_{L1} is approximately out of phase with i_{L2} . The high-frequency current harmonics in i_{L2} is due to the non-ideal operation of the auxiliary circuit, which appears at the DC-link current i_{AB} . The slight phase shift is due to the absorbed active power for the power loss compensation of the auxiliary circuit. With a comparative analysis, the cost, volume and weight of the active inductor is 80.6 %, 68.6 % and 70.7 % of the passive inductor L_p . The reliability comparison is still an open question. It could be a challenge in achieving the same level reliability performance, due to the fact that magnetic components are relatively more reliable than active switching devices and capacitors. Nevertheless, it is not necessarily an issue for practical applications due to the added auxiliary circuit is nothing special compared to a typical full-bridge inverter, which could fulfill the reliability requirement for majority of the industry applications through a proper design.

IV. CONCLUSION

This paper proposes a two-terminal active inductor concept with a minimum apparent power for the auxiliary circuit. It enables a plug-and-play solution without any additional efforts compared to a conventional passive inductor. A current control strategy is applied based on internal feedback signals from the auxiliary circuit only. The key component parameters, energy storage, and the apparent power of the auxiliary active circuit are analyzed. In the case study, the implemented active inductor achieves almost an equivalent impedance curve to a 28 mH passive inductor at the frequencies of interest, while with 27.5% rated inductive energy storage and 21% apparent power compared to the existing solutions shown in Fig. 2 (a).

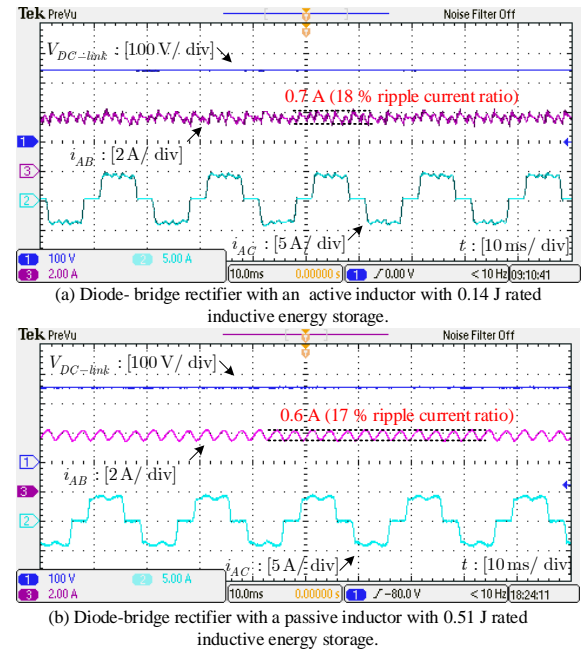


Fig. 7. Experimental waveforms with the passive inductor and the active inductor in the DC link of the three-phase diode-bridge rectifier.

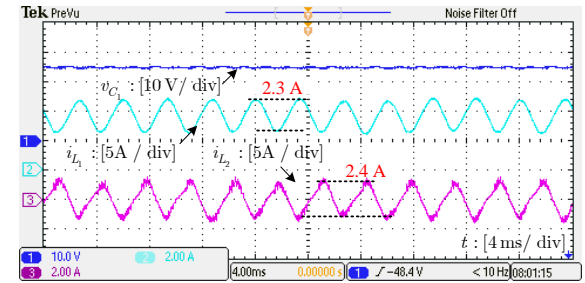


Fig. 8. Experimental waveforms of the active inductor in the case study.

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